

METHOD AND SYSTEM FOR IMPROVING AMPLIFIER EFFICIENCY

TECHNICAL FIELD OF THE INVENTION

This invention relates generally to the field of amplifier circuits and more particularly to a method and system for improving amplifier efficiency.

BACKGROUND OF THE INVENTION

Amplifiers are used to increase or decrease voltage levels in many applications. Proper amplifier design, whether within discrete or integrated circuits, often involves tradeoffs of amplifier characteristics such as efficiency and distortion. Thus, in many applications where low distortion is desirable, performance may suffer from low amplifier efficiency.

Conventional amplifiers, including audio amplifiers, may employ a plurality of stages in order to improve amplifier performance. For example, some amplifier designs may utilize both an input stage that features characteristics such as low distortion and an output stage that resembles a class D stage that typically features higher efficiency. Such a combination may improve the total efficiency of the amplifier. However, such conventional designs may not sufficiently improve amplifier efficiency to meet a desired level of performance. For example, these conventional designs may still suffer from low signal-to-noise ratios and/or dynamic range. Therefore, it is desirable to provide a mechanism for improving amplifier efficiency while maintaining low distortion.

SUMMARY OF THE INVENTION

From the foregoing, it may be appreciated that a need has arisen for providing a system and method to improve efficiency for amplifier applications. In accordance with the present invention, a system and method are provided that substantially eliminate or reduce disadvantages and problems of conventional amplifier systems.

According to an embodiment of the present invention, there is provided an amplifier with an input stage amplifier coupled to an output node. The amplifier includes a class D output stage having at least two switching elements and coupled to the output node. The amplifier also includes a control circuit coupled to the output stage. The control circuit is operable to produce a tri-state output of the output stage in response to a sensed value proportional to an amount of current that flows to the output node. More specifically, the amplifier may comprise an audio amplifier. In another embodiment of the invention, the input stage amplifier may comprise a class AB amplifier.

The invention provides various technical advantages over conventional amplifier systems. Various embodiments of the invention may have none, some, or all of these advantages. For example, one technical advantage is to reduce switching losses of amplifiers, both in systems comprising discrete components and in integrated circuits. This advantage may increase the signal-to-noise ratio and the dynamic range of the amplifier. Another technical advantage may also be reducing electromagnetic interference of the amplifier. Yet

another technical advantage may be improved power consumption over amplifiers utilizing conventional approaches. Other technical advantages may be readily ascertainable by those skilled in the art from the following figures, description, and claims.

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system;
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demonstrating the operation of the amplifier system.

DETAILED DESCRIPTION OF THE INVENTION

FIGURE 1 illustrates a block diagram of an amplifier system 10. Amplifier 10 includes an input stage amplifier 20 coupled to an input voltage V_{IN} , a threshold circuit 30 and an output load 80. Amplifier system 10 also includes a control circuit 40 coupled to threshold circuit 30 and to output stage 50. Output stage 50 is also coupled to output load 80. Although direct connections are illustrated for various elements, many elements may be coupled through other elements without departing from the scope of the invention. As further detailed below, control circuit 40 may be coupled to and may control any class D output stage 50. Control circuit 40 is operable to control the current flowing to output load 80 by activating and deactivating switches within output stage 50 in response to a measured value that senses the amount of current flowing to output load 80. Such control of current flowing to output load 80 may improve the efficiency of amplifier system 10.

Input stage amplifier 20 controls a voltage at output node 81 and provides a current I_o to output load 80. Input stage amplifier 20 may include any suitable input amplifier stage operable to provide current I_o to output load 80. For example, in audio applications where low distortion may be desirable, input stage amplifier 20 may comprise a class A or class AB input stage amplifier, and/or output load 80 may comprise an audio speaker.

Threshold circuit 30 senses the current I_o flowing to output load 80 from input stage amplifier 20 and produces a sensed value. Current I_o may be represented as a positive current as it flows from input stage 20 to

output load 80 and a negative current in the opposite direction. Threshold circuit 30 may include one or multiple stages with a response time suitable for closed loop control of output stage 50. In one embodiment of the invention, threshold circuit 30 may include an adjustable threshold used to generate the sensed value.

In response to the sensed value, control circuit 40 controls the current I_o flowing to output load 80 by activating and deactivating switches within output stage 50. Control circuit 40 includes logic to generate a control signal that controls output stage 50 in response to the sensed value. Output stage 50 may include any switching, or class D, stage suitable to drive output load 80. Any types of switching elements may be used in output stage 50. In this embodiment and as is described below, output stage 50 includes MOSFET switches P1 and N1.

In operation, the magnitude and direction of current I_o as measured at output node 81 may vary as a function of voltage input V_{IN} . Control circuit 40 operates to control current I_o by providing tri-state control of the switches within output stage 50. For example, control circuit 40 may desirably deactivate both switches P1 and N1 for any current I_o whose magnitude drops below a desired threshold. Where the magnitude of negative current I_o exceeds such a threshold, control circuit 40 activates switch N1 and deactivates switch P1. Similarly, where the magnitude of positive current I_o exceeds the threshold, control circuit 40 activates switch P1 and deactivates switch N1. The switches in output stage 50 are thus controlled so that output stage 50 comprises

three possible states, or on-off-on, as a function of current I_o . Such control may advantageously dissipate little or no power through switches P1 and N1 when current I_o diminishes to approximately zero. Threshold circuit 30 and control circuit 40 may utilize any configuration and threshold suitable to achieve such tri-state control within the closed loop delay for current I_o to travel from input stage amplifier 20 to output load 80.

FIGURE 2 illustrates an exemplary schematic diagram of amplifier system 10 utilizing the teachings of the present invention. Amplifier system 10 includes input amplifier stage 20, threshold circuit 30, control circuit 40, and output load 80, as is discussed in conjunction with FIGURE 1. Although direct connections are illustrated for various elements, many elements may be coupled through other elements without departing from the scope of the invention. Amplifier system 10 may be an integrated circuit or discrete components.

In this embodiment, input amplifier stage 20 is designed as a class AB input stage amplifier coupled to voltage input V_{IN} . Input amplifier stage 20 is configured with gain suitable to couple to a resistive output load 80 such as an audio speaker. In this embodiment, input amplifier stage 20 also includes a sense resistor R_{sense} coupled to output node 81 through which current I_o flows to output load 80. Threshold circuit 30 couples to input stage amplifier 20 at each end of resistor R_{sense} . Threshold circuit 30 may also couple to resistors internal to input stage amplifier 20.

Output stage 50 has a p-channel MOSFET switch P1 and an n-channel MOSFET switch N1. The drains of switches P1 and N1 are each coupled to output load 80 through an inductor L1. Inductor L1 stores energy transferred from switches P1 and N1 and isolates output stage 50 from input stage amplifier 20. As discussed in further detail below, control circuit 40 may be used to activate and deactivate switches P1 and N1 to control current flow to output load 80.

In this embodiment, output load 80 is designed as an audio speaker. Control circuit 40 may be used to deactivate switches P1 and N1 for small signal output levels. Such an advantage may reduce electromagnetic interference, switching losses, and lower the noise floor for small signal output levels. Output loads that may require inductive coupling to output stage 50, such as motors, may also be used. Other output loads 80 that may be driven by output stage 50, with or without inductor L1, are also within the scope of the invention.

Threshold circuit 30 has a differential amplifier 32 coupled to threshold adjustor 34 at node 33. Threshold circuit 30 is coupled to control circuit 40 at node 41. Differential amplifier 32 is configured with a gain suitable to amplify the voltage potential V_R across resistor R_{sense} and to produce an amplified voltage potential V_A at node 33. In response to potential V_A at node 33, threshold adjustor 34 is configured with a gain suitable to produce at node 41 a sensed value, voltage V_P , that is proportional to current I_O . Threshold adjustor 34 may also produce an adjustable voltage V_P at node 41 by utilizing an adjustable gain configuration. For example,

threshold adjustor 34 may use adjustable resistors or may be designed in fewer or more stages. For example, threshold circuit 30 may comprise a plurality of cascaded stages where more gain may be desirable. Other threshold
5 circuits 30, including current mirrors and differential amplifiers, may also be used to sense current I_0 and to produce a sensed value therefrom, and are within the scope of the invention.

In this embodiment, control circuit 40 comprises two
10 generally symmetric portions 42 and 44. For example, portion 42 couples to switch P1 of output stage 50 and uses comparators CP1 and CP2, a resistor divider R1 and R2, and diode DP. Portion 42 is responsive to a positive current I_0 , when current is flowing from input stage 20 to
15 output load 80. Portion 42 operates to activate switch P1 when positive current I_0 exceeds a positive threshold I_{TH} . Portion 42 operates to deactivate switch P1 when positive current I_0 diminishes below another threshold V_{MR} . For example, portion 42 may deactivate switch P1
20 when positive current I_0 reaches approximately zero. Comparators CP1 and CP2 are latch comparators with a Q and Q' output and whose positive reference nodes are each coupled to node 41. The Q' output of comparator CP2 drives the gate of switch P1.

25 The Q output of comparator CP1 couples to the latch input of comparator CP2 and to diode DP. A resistor divider formed by resistors R1 and R2 couples to reference voltages V_{CC} and V_{dd} to provide a suitable threshold voltage V_{TH} for comparator CP2. In this
30 embodiment, voltage V_{TH} has a predetermined value that may be represented by the relationship:

$$V_{TH} = V_{dd} + (V_{cc} - V_{dd}) * R2 / (R2 + R1)$$

Voltage V_{TH} and resistors $R1$ and $R2$ may also be adjustable.

5 In operation, portion 42 of control circuit 40 may control switch $P1$ by activating and deactivating switch $P1$. In this embodiment, portion 42 activates p-channel MOSFET $P1$ when output Q' of comparator $CP2$ is asserted low, and deactivates switch $P1$ when output Q' of comparator $CP2$ is asserted high. In this embodiment,
10 portion 42 activates switch $P1$ only after voltage V_p at node 41 has exceeded reference threshold V_{TH} and until voltage V_p decreases to reference threshold V_{MR} . In this embodiment, reference threshold V_{MR} represents a predetermined value at the general midpoint between a
15 high threshold V_{TH} and a low threshold $-V_{TH}$, and is approximately equal to zero volts. Such control of switch $P1$ desirably reduces any losses through switch $P1$ for small positive currents I_o . Reducing any losses through switch $P1$ desirably reduces noise and electromagnetic
20 interference, and thus increases the signal-to-noise ratio of amplifier 10.

To illustrate, comparator $CP1$ determines when voltage V_p exceeds reference threshold V_{MR} . Comparator $CP1$ will remain asserted high while the voltage at node 41
25 remains above reference threshold V_{MR} . Comparator $CP2$ monitors the voltage V_p at node 41 against reference threshold V_{TH} . The Q output of comparator $CP2$ is asserted high only when voltage V_p exceeds reference threshold V_{TH} . As voltage V_p drops below V_{TH} but remains above V_{MR} , the
30 latch signal from comparator $CP1$, now unblocked by diode DP , latches comparator $CP2$ in the logic high state.

Thus, once V_P exceeds reference threshold V_{TH} , output Q' of comparator CP2 will activate switch P1 as long as voltage V_P remains above V_{MR} . However, as voltage V_P drops below V_{MR} , output Q' is asserted low and thus deactivates switch P1. These voltage waveforms and their relationships are illustrated and discussed in further detail in conjunction with FIGURE 3.

Portion 44 similarly couples to switch N1 of output stage 50 and includes comparators CN1 and CN2, another resistor divider R3 and R4, and diode DN. Portion 44 is responsive to a negative current I_o which flows from output load 80 to input stage 20. Portion 44 operates to activate switch N1 when negative current I_o exceeds a negative threshold $-I_{TH}$ and to subsequently deactivate switch N1 when negative current I_o reaches approximately zero. Comparators CN1 and CN2 are latch comparators with a Q and Q' output and whose negative reference nodes are each coupled to node 41. The Q output of comparator CN2 drives the gate of switch N1.

The Q output of comparator CN1 couples to the latch input of comparator CN2 and to diode DN. Resistors R3 and R4 are coupled to reference voltage V_{dd} and ground to form this resistor divider in order to provide a suitable threshold voltage $-V_{TH}$ for comparator CN2. In this embodiment, $-V_{TH}$ has a predetermined value that may be represented by the relationship:

$$-V_{TH} = V_{dd} * R4 / (R3 + R4)$$

Voltage $-V_{TH}$ and resistors R3 and R4 may also be adjustable.

In operation, portion 44 may control switch N1 by activating and deactivating switch N1. In this

embodiment, portion 44 activates n-channel MOSFET N1 when output Q of comparator CN2 is asserted high, and deactivates switch N1 when output Q of comparator CN2 is asserted low. In this embodiment, portion 44 activates switch N1 only after voltage V_P at node 41 has dropped below reference threshold $-V_{TH}$ and until voltage V_P increases to reference threshold V_{MR} . Such control of switch N1 desirably reduces any losses through switch N1 for small negative currents I_0 . Reducing any losses through switch N1 also desirably reduces noise and electromagnetic interference, and thus increases the signal-to-noise ratio of amplifier 10.

Comparators CN1 and CN2 monitor voltage V_P , and comparator CN1 determines when voltage V_P drops below reference threshold V_{MR} . Comparator CN1 will remain asserted high while voltage V_P remains below reference threshold V_{MR} . The Q output of comparator CN2 is asserted high only when voltage V_P drops below reference threshold $-V_{TH}$. As voltage V_P rises above $-V_{TH}$ but remains below V_{MR} , the latch signal from comparator CN1, now unblocked by diode DN, latches comparator CN2 in the logic high state. Thus, once V_P drops below reference threshold $-V_{TH}$, comparator CN2 will activate switch N1, as long as voltage V_P remains below V_{MR} . However, as voltage V_P rises above V_{MR} , comparator CN2 is latched off and thus deactivates switch P1.

In this way, portions 42 and 44 of control circuit 40 combine to produce a tri-state, or on-off-on, output for output stage 50. Control circuit 40 controls output stage 50 utilizing voltage V_P which is proportional to the magnitude of current I_0 . Control circuit 40 deactivates

both switches P1 and N1 when voltage V_P rises from V_{MR} until it reaches reference threshold V_{TH} , and when voltage V_P decreases from V_{MR} until it reaches reference threshold $-V_{TH}$. Once voltage V_P exceeds reference threshold V_{TH} ,
5 control circuit 40 activates switch P1. Control circuit 40 deactivates switch P1 only when voltage V_P drops to V_{MR} . Similarly, switch N1 is on, and switch P1 is off, once the voltage V_P exceeds reference threshold $-V_{TH}$. Control circuit 40 deactivates switch N1 only when voltage V_P rises to V_{MR} .
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Other reference thresholds V_{MR} , which are proportional to current I_0 , may also be used to control output stage 50 in response to current I_0 . For example, V_{MR} may comprise two suitable non-zero thresholds V_{MRA} and $-V_{MRB}$, that are less than reference thresholds V_{TH} and $-V_{TH}$, respectively. Such non-zero thresholds may accommodate the closed loop delay from resistor R_{sense} to output stage 50. For example, such non-zero thresholds may desirably ensure that switches P1 and N1 are timely deactivated where current I_0 is decreasing and measures a magnitude near-zero. Propagation or other delays do not prevent switches P1 and N1 from being timely deactivated to generally coincide when current I_0 is approximately zero. Such non-zero thresholds may also be similarly utilized for controlling switches P1 and N1 for generally non-zero currents I_0 .
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Reference thresholds V_{MRA} and $-V_{MRB}$ also may or may not be identical for portions 42 and 44. Other reference thresholds V_{TH} and $-V_{TH}$, which are proportional to current I_0 , may be used as desired. For example, in audio applications, V_{TH} may be used to deactivate switches P1
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and N1 when current I_0 drops below a listener's aural threshold. Furthermore, reference thresholds V_{TH} and $-V_{TH}$ may or may not have identical magnitudes, such as for applications where thresholds for positive and negative currents may desirably differ.

Control circuit 40 may also comprise any logic suitable for producing a tri-state output for output stage 50 in response to current I_0 . For example, control circuit 40 may comprise a current-steering mechanism that may be used with any suitable threshold circuit 30, as discussed above.

FIGURE 3 illustrates a series of waveforms demonstrating the operation of the present invention. Waveforms V1, V2, and V3 are measurable at nodes 41, 42A and 42B, respectively, as described in detail in conjunction with FIGURES 1 and 2. More specifically, waveforms V1, V2, and V3 describe the operation of portion 42 of control circuit 40. As discussed in conjunction with FIGURE 2, portion 42 is responsive to changes in positive current I_0 . The operation of portion 44 of control circuit 40 is not explicitly shown, but may be similarly illustrated, as is discussed below.

Waveform V1 illustrates the voltage level V_p measurable at node 41 which is proportional to the voltage at output node 32 and thus current I_0 . In the embodiment of FIGURE 1, waveform V1 illustrates a typical output for a self-oscillating class D output stage coupled to an inductor between predetermined voltage reference thresholds $-V_{TH}$ and V_{TH} . In this embodiment, V_{MR} represents the midpoint between reference thresholds $-V_{TH}$ and V_{TH} . Voltage thresholds V_{MR} and V_{TH} may be any

suitable thresholds, whether predetermined or dynamically determined. For example, in many audio applications, V_{MR} may be zero.

Waveforms V2 and V3 illustrate the change in logic high and low levels in response to changes in voltage V_p at nodes 42A and 42B, respectively. As discussed in conjunction with FIGURE 2, the logic level at node 42A follows the output of comparator CP1, while the logic level at node 42A follows the outputs of diode DP and comparator CP2. As voltage V_p exceeds reference threshold voltage V_{MR} , comparator CP1 is set and reset, respectively. Thus, waveform V2 remains at an asserted high as long as voltage V_p remains above reference threshold V_{MR} .

Waveform V3 illustrates the Q output of comparator CP2 at node 42B and reflects control latching by comparator CP1. Thus, switch P1 is activated when waveform V3 is at a logic high, because switch P1 is activated by a logic low from the Q' output of comparator CP2. Diode DP prevents comparator CP1 from latching comparator CP2 until the voltage exceeds reference threshold V_{TH} . Waveform V3 is then latched high by comparator CP1 as long as voltage V_p remains above reference threshold V_{MR} . Comparator CP2 then follows waveform V2 as it drops when comparator CP1 is reset as voltage V_p drops below reference threshold V_{MR} .

Portion 44 of control circuit 40 operates similarly to portion 42 and, as discussed in conjunction with FIGURE 2, portion 42 is responsive to changes in negative current I_o . Thus, for example, similar waveforms V2' and V3' (not explicitly shown) would activate switch N1 where

voltage V_p is below reference threshold $-V_{TH}$, and deactivate switch N1 where voltage V_p reaches reference threshold V_{MR} .

5 In this embodiment, V_{MR} is located generally at a midpoint between V_{TH} and $-V_{TH}$. As discussed above, a suitable reference threshold V_{MRA} may be located between such a midpoint and V_{TH} , and may accommodate closed-loop delay of current I_0 and various frequency of signals within amplifier 10.

10 Thus, it is apparent that there has been provided in accordance with the present invention, a system and method for improving amplifier efficiency that satisfies the advantages set forth above. Although the present invention has been described in detail, various changes,
15 substitutions, and alterations may be readily ascertainable by those skilled in the art and may be made herein without departing from the spirit and scope of the present invention as defined by the following claims.